National Semiconductor

January 2007

LM4910 Boomer® Audio Power Amplifier Series
Output Capacitor-less Stereo 35mW Headphone Amplifier

General Description

The LM4910 is an audio power amplifier primarily designed for headphone applications in portable device applications. It is capable of delivering 35mW of continuous average power to a 32Ω load with less than 1% distortion (THD+N) from a $3.3V_{DC}$ power supply.

The LM4910 utilizes a new circuit topology that eliminates output coupling capacitors and half-supply bypass capacitors. The LM4910 contains advanced pop & click circuitry which eliminates noises caused by transients that would otherwise occur during turn-on and turn-off.

Boomer audio power amplifiers were designed specifically to provide high quality output power with a minimal amount of external components. Since the LM4910 does not require any output coupling capacitors, half-supply bypass capacitors, or bootstrap capacitors, it is ideally suited for low-power portable applications where minimal space and power consumption are primary requirements.

The LM4910 features a low-power consumption shutdown mode, activated by driving the shutdown pin with logic low. Additionally, the LM4910 features an internal thermal shutdown protection mechanism. The LM4910 is also unity-gain stable and can be configured by external gain-setting resistors.

Key Specifications

- PSRR at f = 217Hz — 65dB (typ)
- Power Output at V_{DD} = 3.3V, R_L = 32Ω, and THD ≤ 1% — 35mW (typ)
- Shutdown Current — 0.1µA (typ)

Features

- Eliminates headphone amplifier output coupling capacitors
- Eliminates half-supply bypass capacitor
- Advanced pop & click circuitry eliminates noises during turn-on and turn-off
- Ultra-low current shutdown mode
- Unity-gain stable
- 2.2V - 5.5V operation
- Available in space-saving MSOP, LLP, and SOIC packages

Applications

- Mobile Phones
- PDAs
- Portable electronics devices
- Portable MP3 players

Typical Application

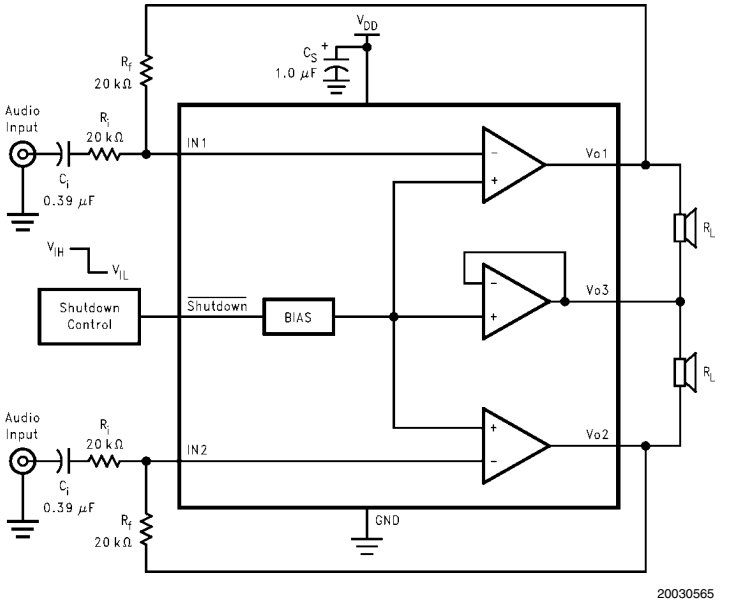

FIGURE 1. Typical Audio Amplifier Application Circuit

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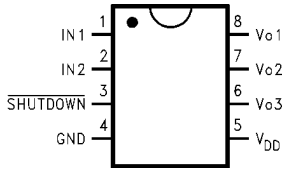
Connection Diagrams

MSOP/SO Package



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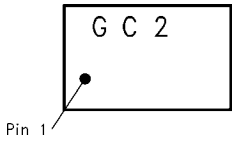
Top View
Order Number LM4910MM or LM4910MA
See NS Package Number MUA08A or M08A

MSOP Marking



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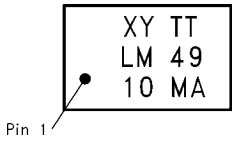
Top View
G - Boomer Family
C2 - LM4910MM

SO Marking



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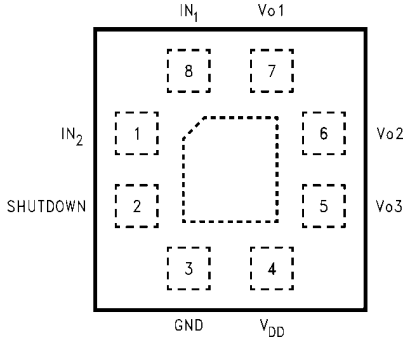
Top View
TT - Die Traceability
Bottom 2 lines - Part Number

LLP Package



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Top View
Order Number LM4910LQ
See NS package Number LQB08A

Absolute Maximum Ratings (Note 2)

If Military/Aerospace specified devices are required, please contact the National Semiconductor Sales Office/ Distributors for availability and specifications.

Supply Voltage (Note 9)	6.0V
Storage Temperature	−65°C to +150°C
Input Voltage	-0.3V to V_{DD} + 0.3V
Power Dissipation (Note 3)	Internally Limited
ESD Susceptibility Pin 6 (Note 10)	10kV
ESD Susceptibility (Note 4)	2000V
ESD Susceptibility (Note 5)	200V
Junction Temperature	150°C
Thermal Resistance	
θ_{JC} (MSOP)	56°C/W
θ_{JA} (MSOP)	190°C/W
θ_{JC} (SOP)	35°C/W
θ_{JA} (SOP)	150°C/W
θ_{JC} (LQ)	57°C/W
θ_{JA} (LQ)	140°C/W

Operating Ratings

Temperature Range	
$T_{MIN} \le T_A \le T_{MAX}$	$-40°C \le T_A \le 85°C$
Supply Voltage (V_{DD})	$2.2V \le V_{CC} \le 5.5V$

Electrical Characteristics V_{DD} = 3.3V (Notes 1, 2)

The following specifications apply for V_{DD} = 3.3V, A_V = 1, and 32Ω load unless otherwise specified. Limits apply to T_A = 25°C.

Symbol	Parameter	Conditions	LM4910		Units (Limits)
			Typ (Note 6)	Limit (Notes 7, 8)	
I_{DD}	Quiescent Power Supply Current	V_{IN} = 0V, 32Ω Load	3.5	6	mA (max)
I_{SD}	Standby Current	$V_{SHUTDOWN}$ = GND	0.1	1.0	µA (max)
V_{OS}	Output Offset Voltage		5	30	mV (max)
P_O	Output Power	THD = 1% (max); f = 1kHz	35	30	mW (min)
THD+N	Total Harmonic Distortion + Noise	P_O = 30mW_{rms}; f = 1kHz	0.3		%
PSRR	Power Supply Rejection Ratio	V_{RIPPLE} = 200mV_{p-p} sinewave Input terminated with 10Ω to ground	65 (f = 217Hz) 65 (f = 1kHz)		dB
V_{IH}	Shutdown Input Voltage High			1.5	V (min)
V_{IL}	Shutdown Input Voltage Low			0.4	V (max)

Electrical Characteristics V_{DD} = 3V (Notes 1, 2)

The following specifications apply for V_{DD} = 3V, A_V = 1, and 32Ω load unless otherwise specified. Limits apply to T_A = 25°C.

Symbol	Parameter	Conditions	LM4910		Units (Limits)
			Typ (Note 6)	Limit (Notes 7, 8)	
I_{DD}	Quiescent Power Supply Current	V_{IN} = 0V, 32Ω Load	3.3	6	mA (max)
I_{SD}	Standby Current	$V_{SHUTDOWN}$ = GND	0.1	1.0	µA (max)
V_{OS}	Output Offset Voltage		5	30	mV (max)
P_O	Output Power	THD = 1% (max); f = 1kHz	30	25	mW (min)
THD+N	Total Harmonic Distortion + Noise	P_O = 25mW_{rms}; f = 1kHz	0.3		%
PSRR	Power Supply Rejection Ratio	V_{RIPPLE} = 200mV_{p-p} sinewave Input terminated with 10Ω to ground	65 (f = 217 Hz) 65 (f = 1kHz)		dB
V_{IH}	Shutdown Input Voltage High			1.5	V (min)
V_{IL}	Shutdown Input Voltage Low			0.4	V (max)

Electrical Characteristics V_{DD} = 2.6V (Notes 1, 2)

The following specifications apply for V_{DD} = 2.6V, A_V = 1, and 32Ω load unless otherwise specified. Limits apply to T_A = 25°C.

Symbol	Parameter	Conditions	LM4910		Units (Limits)
			Typ (Note 6)	Limit (Notes 7, 8)	
I_{DD}	Quiescent Power Supply Current	V_{IN} = 0V, 32Ω Load	3.0		mA (max)
I_{SD}	Standby Current	$V_{SHUTDOWN}$ = GND	0.1		µA (max)
V_{OS}	Output Offset Voltage		5		mV (max)
P_O	Output Power	THD = 1% (max); f = 1kHz	13		mW
THD+N	Total Harmonic Distortion + Noise	P_O = 10mW_{rms}; f = 1kHz	0.3		%
PSRR	Power Supply Rejection Ratio	V_{RIPPLE} = 200mV_{p-p} sinewave Input terminated with 10Ω to ground	55 (f = 217Hz) 55 (f = 1kHz)		dB

Note 1: All voltages are measured with respect to the GND pin unless otherwise specified.

Note 2: Absolute Maximum Ratings indicate limits beyond which damage to the device may occur. Operating Ratings indicate conditions for which the device is functional but do not guarantee specific performance limits. Electrical Characteristics state DC and AC electrical specifications under particular test conditions which guarantee specific performance limits. This assumes that the device is within the Operating Ratings. Specifications are not guaranteed for parameters where no limit is given, however, the typical value is a good indication of device performance.

Note 3: The maximum power dissipation must be derated at elevated temperatures and is dictated by T_{JMAX}, θ_{JA}, and the ambient temperature, T_A. The maximum allowable power dissipation is $P_{DMAX} = (T_{JMAX} - T_A)/\theta_{JA}$ or the number given in Absolute Maximum Ratings, whichever is lower. For the LM4910, see power derating currents for more information.

Note 4: Human body model, 100pF discharged through a 1.5kΩ resistor.

Note 5: Machine Model, 220pF-240pF discharged through all pins.

Note 6: Typicals are measured at 25°C and represent the parametric norm.

Note 7: Limits are guaranteed to National's AOQL (Average Outgoing Quality Level).

Note 8: Datasheet min/max specification limits are guaranteed by design, test, or statistical analysis.

Note 9: If the product is in shutdown mode and V_{DD} exceeds 6V (to a max of 8V V_{DD}) then most of the excess current will flow through the ESD protection circuits. If the source impedance limits the current to a max of 10ma then the part will be protected. If the part is enabled when V_{DD} is above 6V circuit performance will be curtailed or the part may be permanently damaged.

Note 10: Human body model, 100pF discharged through a 1.5kΩ resistor, Pin 6 to ground.

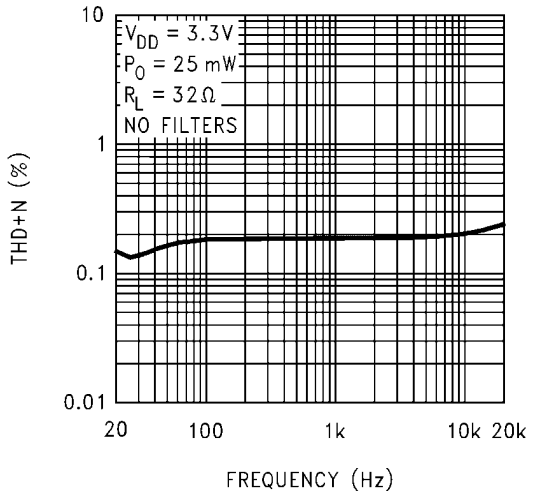
External Components Description

(*Figure 1*)

Components		Functional Description
1.	R_I	Inverting input resistance which sets the closed-loop gain in conjunction with R_f. This resistor also forms a high-pass filter with C_i at $f_c = 1/(2\pi R_i C_i)$.
2.	C_I	Input coupling capacitor which blocks the DC voltage at the amplifier's input terminals. Also creates a high-pass filter with R_i at $f_c = 1/(2\pi R_i C_i)$. Refer to the section **Proper Selection of External Components,** for an explanation of how to determine the value of C_i.
3.	R_f	Feedback resistance which sets the closed-loop gain in conjunction with R_i.
4.	C_S	Supply bypass capacitor which provides power supply filtering. Refer to the **Power Supply Bypassing** section for information concerning proper placement and selection of the supply bypass capacitor.

Typical Performance Characteristics

THD+N vs Frequency



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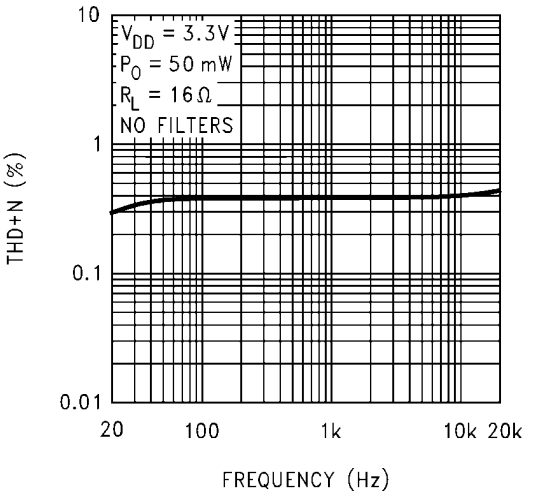
THD+N vs Frequency



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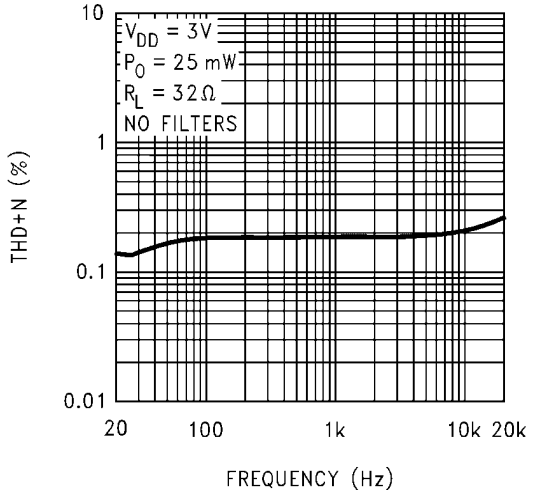
THD+N vs Frequency



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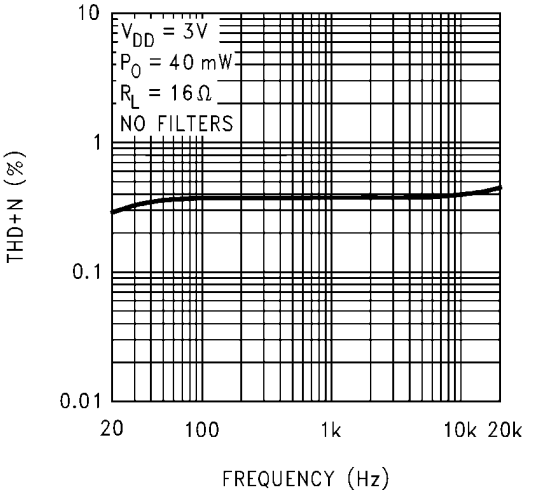
THD+N vs Frequency



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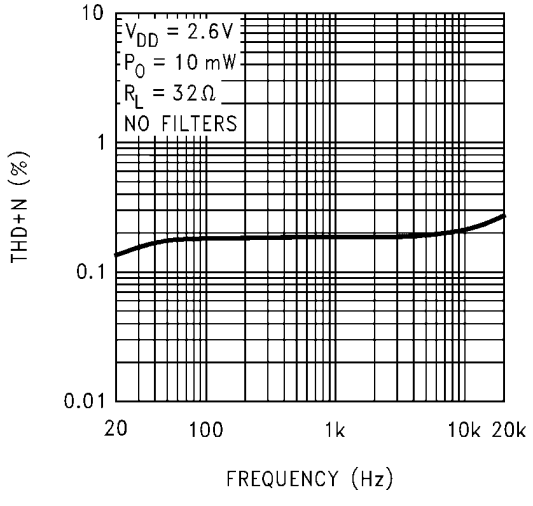
THD+N vs Frequency



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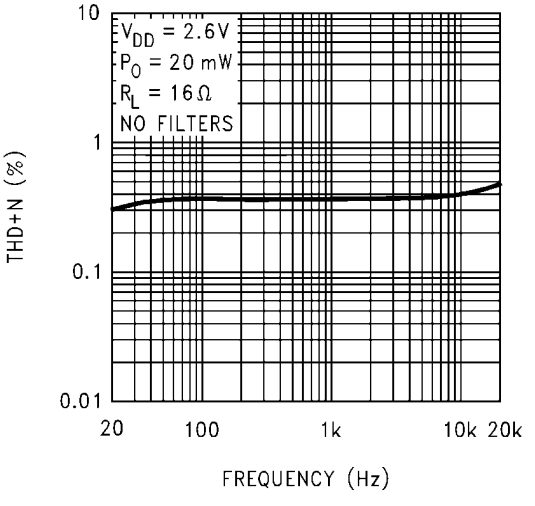
THD+N vs Frequency



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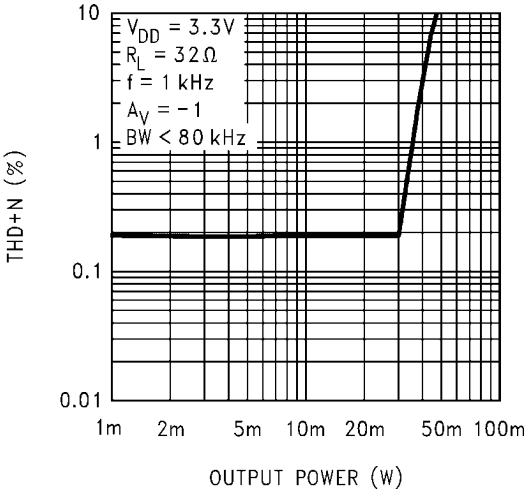
THD+N vs Output Power



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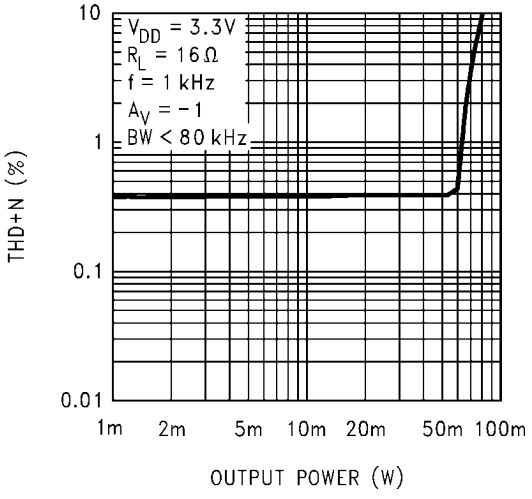
THD+N vs Output Power



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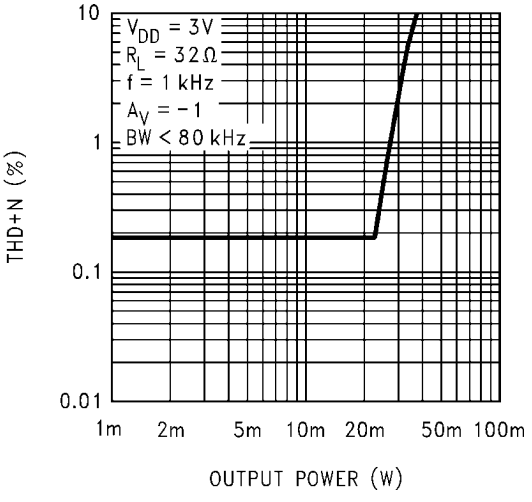
THD+N vs Output Power



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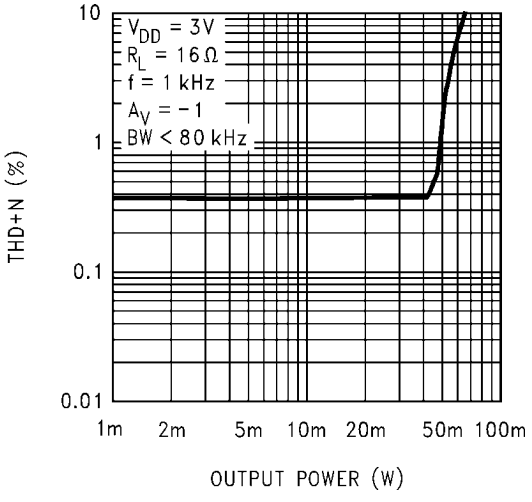
THD+N vs Output Power



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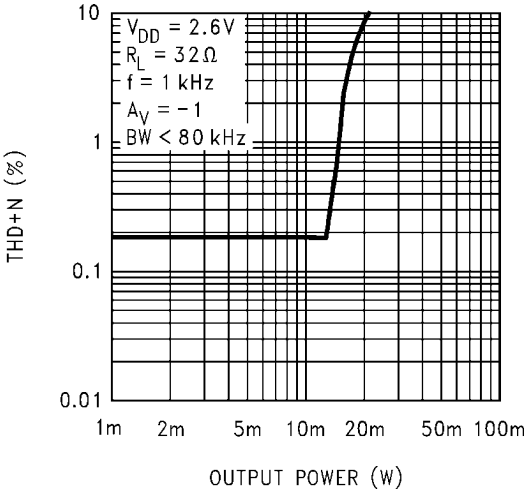
THD+N vs Output Power



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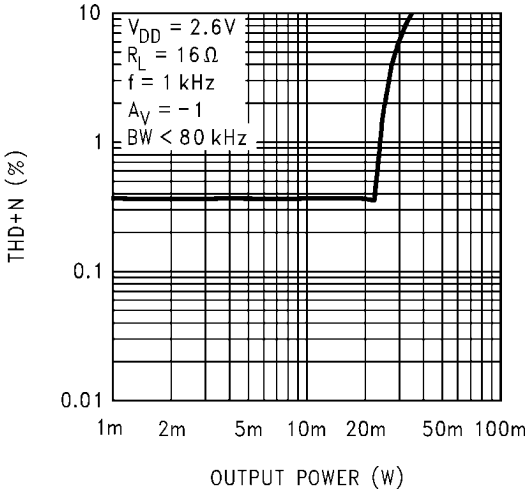
THD+N vs Output Power



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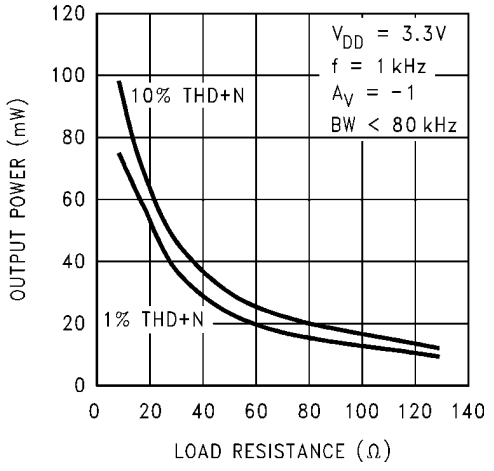
Output Power vs Load Resistance



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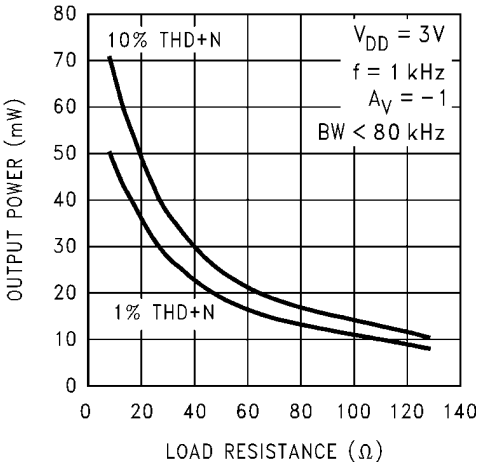
Output Power vs Load Resistance



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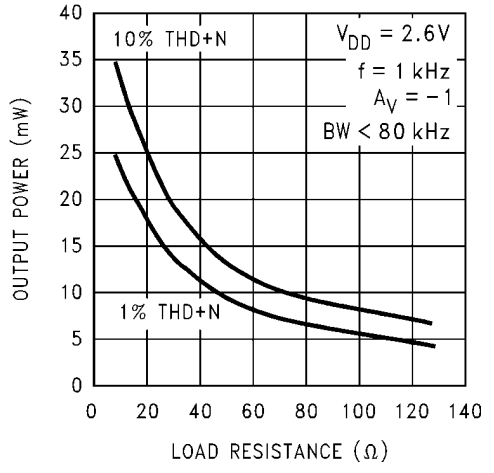
Output Power vs Load Resistance



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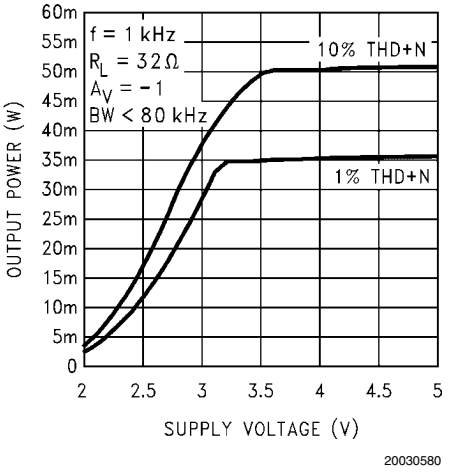
Output Power vs Supply Voltage



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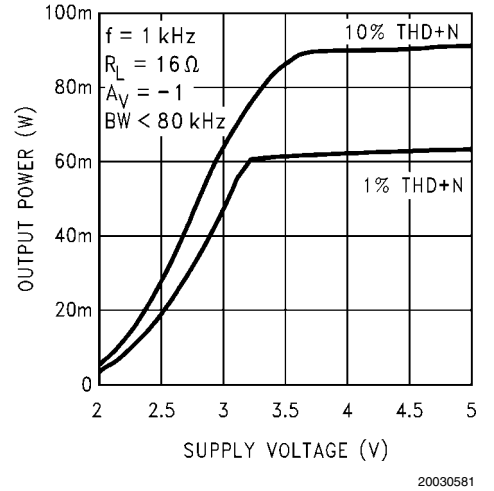
Output Power vs Supply Voltage



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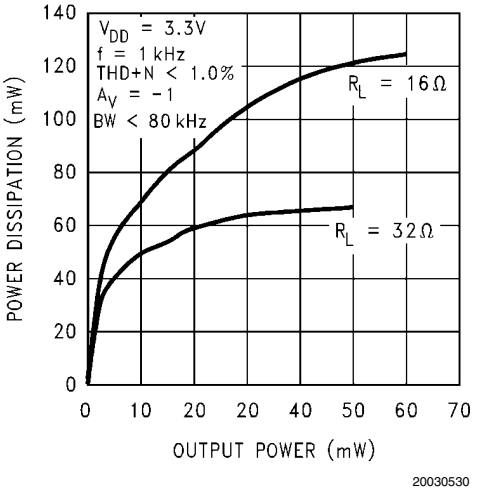
Power Dissipation vs Output Power



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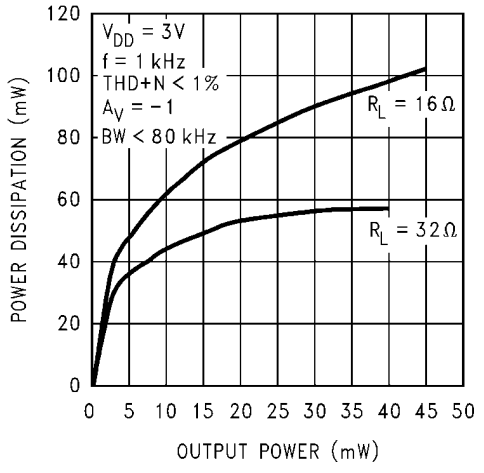
Power Dissipation vs Output Power



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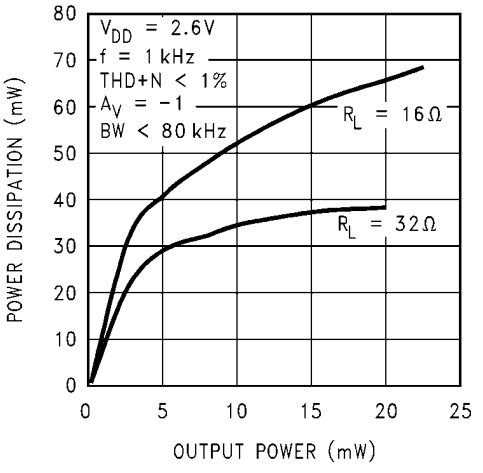
Power Dissipation vs Output Power



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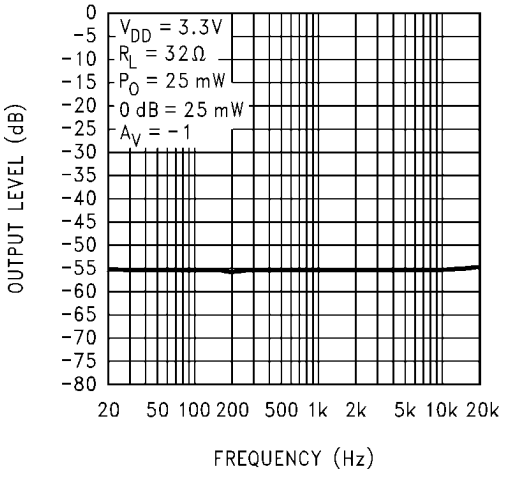
Channel Separation



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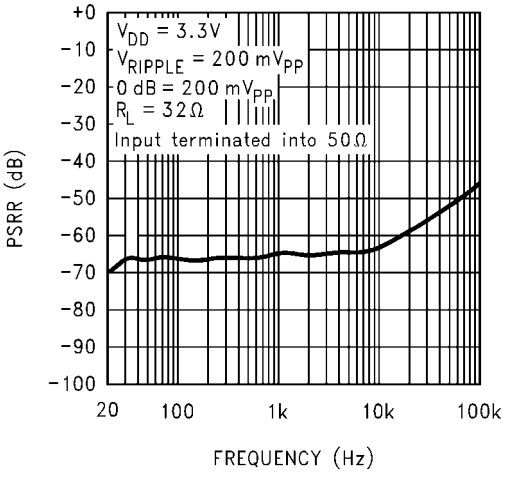
Power Supply Rejection Ratio



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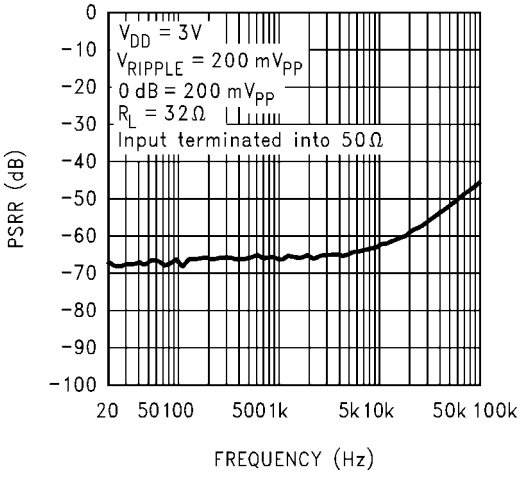
Power Supply Rejection Ratio



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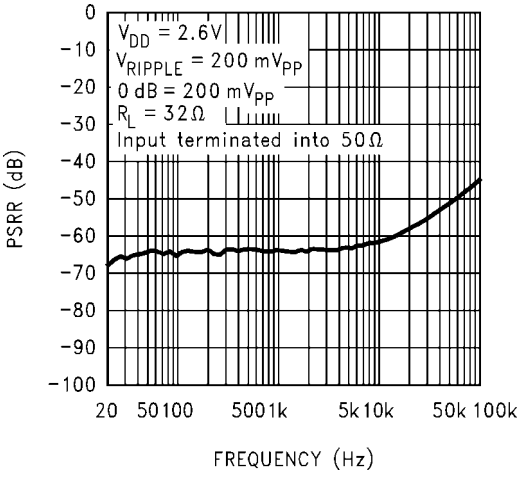
Power Supply Rejection Ratio



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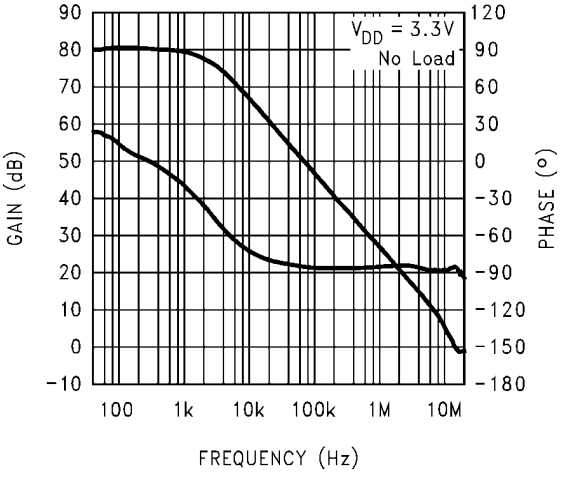
Open Loop Frequency Response



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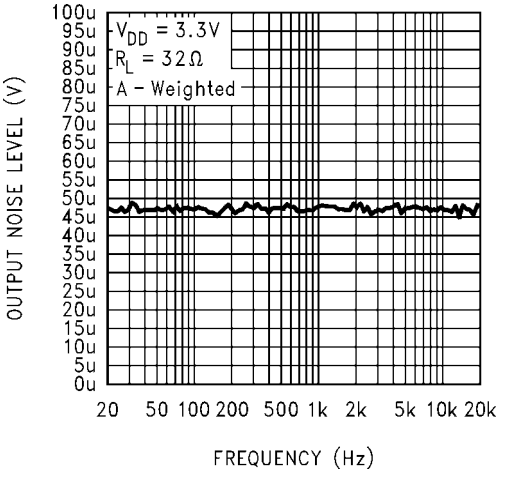
Noise Floor



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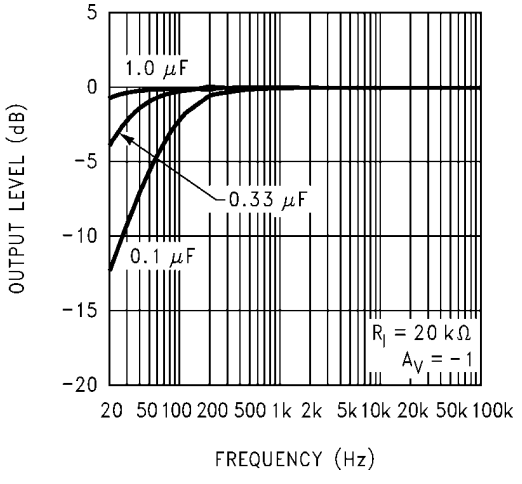
Frequency Response vs Input Capacitor Size



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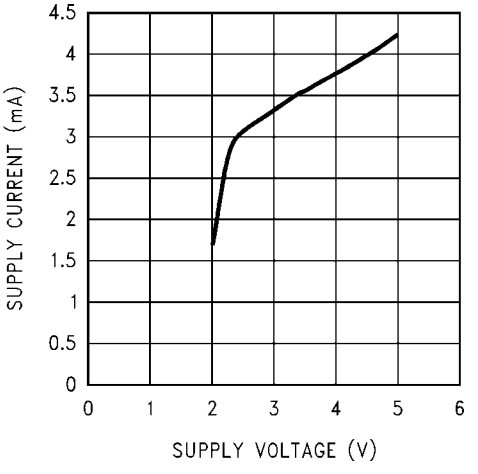
Supply Current vs Supply Voltage



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Application Information

ELIMINATING OUTPUT COUPLING CAPACITORS

Typical single-supply audio amplifiers that drive single-ended (SE) headphones use a coupling capacitor on each SE output. This output coupling capacitor blocks the half-supply voltage to which the output amplifiers are typically biased and couples the audio signal to the headphones. The signal return to circuit ground is through the headphone jack's sleeve.

The LM4910 eliminates these output coupling capacitors. Amp3 is internally configured to apply a bandgap referenced voltage (V_{REF} = 1.58V) to a stereo headphone jack's sleeve. This voltage matches the quiescent voltage present on the Amp1 and Amp2 outputs that drive the headphones. The headphones operate in a manner similar to a bridge-tied-load (BTL). The same DC voltage is applied to both headphone speaker terminals. This results in no net DC current flow through the speaker. AC current flows through a headphone speaker as an audio signal's output amplitude increases on the speaker's terminal.

The headphone jack's sleeve is not connected to circuit ground. Using the headphone output jack as a line-level output will place the LM4910's bandgap referenced voltage on a plug's sleeve connection. This presents no difficulty when the external equipment uses capacitively coupled inputs. For the very small minority of equipment that is DC-coupled, the LM4910 monitors the current supplied by the amplifier that drives the headphone jack's sleeve. If this current exceeds 500mA_{PK}, the amplifier is shutdown, protecting the LM4910 and the external equipment.

ELIMINATING THE HALF-SUPPLY BYPASS CAPACITOR

Typical single-supply audio amplifers are normally biased to 1/2V_{DD} in order to maximize the output swing of the audio signal. This is usually achieved with a simple resistor divider network from V_{DD} to ground that provides the proper bias voltage to the amplifier. However, this scheme requires the use of a half-supply bypass capacitor to improve the bias voltage's stability and the amplifier's PSRR performance.

The LM4910 utilizes an internally generated, buffered bandgap reference voltage as the amplifier's bias voltage. This bandgap reference voltage is not a direct function of V_{DD} and therefore is less susceptible to noise or ripple on the power supply line. This allows for the LM4910 to have a stable bias voltage and excellent PSRR performance even without a half-supply bypass capacitor.

OUTPUT TRANSIENT ('CLICK AND POPS') ELIMINATED

The LM4910 contains advanced circuitry that virtually eliminates output transients ('clicks and pops'). This circuitry prevents all traces of transients when the supply voltage is first applied or when the part resumes operation after coming out of shutdown mode. The LM4910 remains in a muted condition until there is sufficient input signal magnitude (>5mV_{RMS}, typ) to mask any remaining transient that may occur. Figure 2 shows the LM4910's lack of transients in the differential signal (Trace B) across a 320 load. The LM4910's active-low $\overline{\text{SHUTDOWN}}$ pin is driven by the logic signal shown in Trace A. Trace C is the V_{O1} output signal and Trace D is the V_{O3} output signal.

To ensure optimal click and pop performance under low gain configurations (less than 0dB), it is critical to minimize the RC combination of the feedback resistor R_F and stray input capacitance at the amplifier inputs. A more reliable way to lower gain or reduce power delivered to the load is to place a current limiting resistor in series with the load as explained in the **Minimizing Output Noise / Reducing Output Power** section.

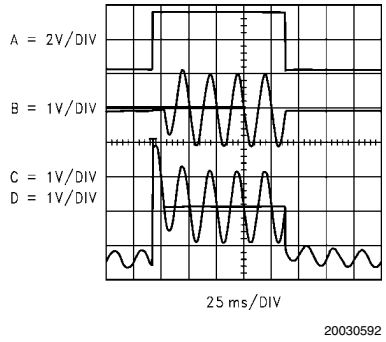


FIGURE 2.

AMPLIFIER CONFIGURATION EXPLANATION

As shown in *Figure 1*, the LM4910 has three operational amplifiers internally. Two of the amplifier's have externally configurable gain while the other amplifier is internally fixed at the bias point acting as a unity-gain buffer. The closed-loop gain of the two configurable amplifiers is set by selecting the ratio of R_f to R_i. Consequently, the gain for each channel of the IC is

$$A_V = -(R_f/R_i)$$

By driving the loads through outputs V_{O1} and V_{O2} with V_{O3} acting as a buffered bias voltage the LM4910 does not require output coupling capacitors. The typical single-ended amplifier configuration where one side of the load is connected to ground requires large, expensive output coupling capacitors.

A configuration such as the one used in the LM4910 has a major advantage over single supply, single-ended amplifiers. Since the outputs V_{O1}, V_{O2}, and V_{O3} are all biased at V_{REF} = 1.58V, no net DC voltage exists across each load. This eliminates the need for output coupling capacitors that are required in a single-supply, single-ended amplifier configuration. Without output coupling capacitors in a typical single-supply, single-ended amplifier, the bias voltage is placed across the load resulting in both increased internal IC power dissipation and possible loudspeaker damage.

POWER DISSIPATION

Power dissipation is a major concern when designing a successful amplifier. A direct consequence of the increased power delivered to the load by a bridge amplifier is an increase in internal power dissipation. The maximum power dissipation for a given application can be derived from the power dissipation graphs or from Equation 1.

$$P_{DMAX} = 4(V_{DD})^2 / (\pi^2 R_L) \quad (1)$$

It is critical that the maximum junction temperature T_{JMAX} of 150°C is not exceeded. Since the typical application is for headphone operation (32Ω impedance) using a 3.3V supply the maximum power dissipation is only 138mW. Therefore, power dissipation is not a major concern.

POWER SUPPLY BYPASSING

As with any amplifier, proper supply bypassing is important for low noise performance and high power supply rejection. The capacitor location on the power supply pins should be as close to the device as possible.

Typical applications employ a 3.3V regulator with 10µF tantalum or electrolytic capacitor and a ceramic bypass capacitor which aid in supply stability. This does not eliminate the need for bypassing the supply nodes of the LM4910. A bypass capacitor value in the range of 0.1µF to 1µF is recommended for C_S.

MICRO POWER SHUTDOWN

The voltage applied to the $\overline{\text{SHUTDOWN}}$ pin controls the LM4910's shutdown function. Activate micro-power shutdown by applying a logic-low voltage to the $\overline{\text{SHUTDOWN}}$ pin. When active, the LM4910's micro-power shutdown feature turns off the amplifier's bias circuitry, reducing the supply current. The trigger point is 0.4V(max) for a logic-low level, and 1.5V(min) for a logic-high level. The low 0.1µA(typ) shutdown current is achieved by applying a voltage that is as near as ground as possible to the $\overline{\text{SHUTDOWN}}$ pin. A voltage that is higher than ground may increase the shutdown current.

There are a few ways to control the micro-power shutdown. These include using a single-pole, single-throw switch, a microprocessor, or a microcontroller. When using a switch, connect an external 100kΩ pull-up resistor between the $\overline{\text{SHUTDOWN}}$ pin and V_{DD}. Connect the switch between the $\overline{\text{SHUTDOWN}}$ pin and ground. Select normal amplifier operation by opening the switch. Closing the switch connects the $\overline{\text{SHUTDOWN}}$ pin to ground, activating micro-power shutdown. The switch and resistor guarantee that the $\overline{\text{SHUTDOWN}}$ pin will not float. This prevents unwanted state changes. In a system with a microprocessor or microcontroller, use a digital output to apply the control voltage to the $\overline{\text{SHUTDOWN}}$ pin. Driving the $\overline{\text{SHUTDOWN}}$ pin with active circuitry eliminates the pull-up resistor.

SELECTING EXTERNAL COMPONENTS

Selecting proper external components in applications using integrated power amplifiers is critical to optimize device and system performance. While the LM4910 is tolerant of external component combinations, consideration to component values must be used to maximize overall system quality.

The LM4910 is unity-gain stable which gives the designer maximum system flexibility. The LM4910 should be used in low gain configurations to minimize THD+N values, and maximize the signal to noise ratio. Low gain configurations require large input signals to obtain a given output power. Input signals equal to or greater than $1V_{rms}$ are available from sources such as audio codecs. Very large values should not be used for the gain-setting resistors. Values for R_i and R_f should be less than 1MΩ. Please refer to the section, **Audio Power Amplifier Design**, for a more complete explanation of proper gain selection

Besides gain, one of the major considerations is the closed-loop bandwidth of the amplifier. To a large extent, the bandwidth is dictated by the choice of external components shown in *Figure 1*. The input coupling capacitor, C_i, forms a first order high pass filter which limits low frequency response. This value should be chosen based on needed frequency response and turn-on time.

SELECTION OF INPUT CAPACITOR SIZE

Amplifiying the lowest audio frequencies requires a high value input coupling capacitor, C_i. A high value capacitor can be expensive and may compromise space efficiency in portable designs. In many cases, however, the headphones used in portable systems have little ability to reproduce signals below 60Hz. Applications using headphones with this limited frequency response reap little improvement by using a high value input capacitor.

In addition to system cost and size, turn-on time is affected by the size of the input coupling capacitor Ci. A larger input coupling capacitor requires more charge to reach its quiescent DC voltage. This charge comes from the output via the feedback Thus, by minimizing the capacitor size based on necessary low frequency response, turn-on time can be minimized. A small value of Ci (in the range of 0.1µF to 0.39µF), is recommended.

USING EXTERNAL POWERED SPEAKERS

The LM4910 is designed specifically for headphone operation. Often the headphone output of a device will be used to drive external powered speakers. The LM4910 has a differential output to eliminate the output coupling capacitors. The result is a headphone jack sleeve that is connected to V_{O3} instead of GND. For powered speakers that are designed to have single-ended signals at the input, the click and pop circuitry will not be able to eliminate the turn-on/turn-off click and pop. Unless the inputs to the powered speakers are fully differential the turn-on/turn-off click and pop will be very large.

AUDIO POWER AMPLIFIER DESIGN

A 30mW/32Ω Audio Amplifier

Given:	
Power Output	30mWrms
Load Impedance	32Ω
Input Level	1Vrms
Input Impedance	20kΩ

A designer must first determine the minimum supply rail to obtain the specified output power. By extrapolating from the Output Power vs Supply Voltage graphs in the **Typical Performance Characteristics** section, the supply rail can be easily found.

Since 3.3V is a standard supply voltage in most applications, it is chosen for the supply rail in this example. Extra supply voltage creates headroom that allows the LM4910 to reproduce peaks in excess of 30mW without producing audible distortion. At this time, the designer must make sure that the power supply choice along with the output impedance does no violate the conditions explained in the **Power Dissipation** section.

Once the power dissipation equations have been addressed, the required differential gain can be determined from Equation 2.

$$A_V \geq \sqrt{(P_O R_L)}/(V_{IN}) = V_{orms}/V_{inrms} \quad (2)$$

From Equation 2, the minimum A_V is 0.98; use $A_V = 1$. Since the desired input impedance is 20kΩ, and with A_V equal to 1, a ratio of 1:1 results from Equation 1 for R_f to R_i. The values are chosen with R_i = 20kΩ and R_f = 20kΩ.

The last step in this design example is setting the amplifier's −3dB frequency bandwidth. To achieve the desired ±0.25dB pass band magnitude variation limit, the low frequency re-

sponse must extend to at least one-fifth the lower bandwidth limit and the high frequency response must extend to at least five times the upper bandwidth limit. The gain variation for both response limits is 0.17dB, well within the ±0.25dB desired limit. The results are an

$$f_L = 100Hz/5 = 20Hz \quad (3)$$

and an

$$f_H = 20kHz \times 5 = 100kHz \quad (4)$$

As mentioned in the **Selecting Proper External Components** section, R_i and C_i create a highpass filter that sets the amplifier's lower bandpass frequency limit. Find the coupling capacitor's value using Equation (3).

$$C_i \geq 1/(2\pi R_i f_L) \quad (5)$$

The result is

$$1/(2\pi * 20k\Omega * 20Hz) = 0.397\mu F$$

Use a 0.39µF capacitor, the closest standard value.

The high frequency pole is determined by the product of the desired frequency pole, f_H, and the differential gain, A_V. With an $A_V = 1$ and $f_H = 100kHz$, the resulting GBWP = 100kHz which is much smaller than the LM4910 GBWP of 11MHz. This figure displays that if a designer has a need to design an amplifier with higher differential gain, the LM4910 can still be used without running into bandwidth limitations.

MINIMIZING OUTPUT NOISE / REDUCING OUTPUT POWER

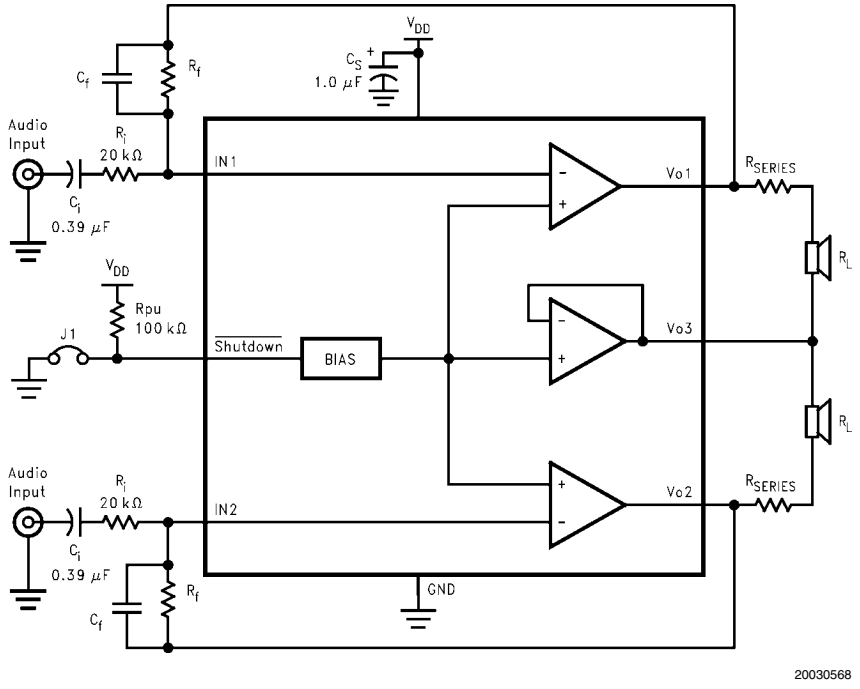


FIGURE 3.

Output noise delivered to the load can be minimized with the use of an external resistor, R_{SERIES}, placed in series with each load as shown in *Figure 3*. R_{SERIES} forms a voltage divider with the impedance of the headphone driver R_L. As a result, output noise is attenuated by the factor $R_L / (R_L + R_{SERIES})$. *Figure 4* illustrates the relationship between output noise and R_{SERIES} for different loads. R_{SERIES} also decreases output power delivered to the load by the factor $R_L / (R_L + R_{SERIES})^2$. However, this may not pose a problem since most headphone applications require less than 10mW of output power. *Figure 5* illustrates output power (@1% THD+N) vs R_{SERIES} for different loads.

Figure 4 shows an optional resistor connected between the amplifier output that drives the headphone jack sleeve and ground. This resistor provides a ground path that supressed power supply hum. This hum may occur in applications such as notebook computers in a shutdown condition and connected to an external powered speaker. The resistor's 100Ω value is a suggested starting point. Its final value must be determined based on the tradeoff between the amount of noise suppression that may be needed and minimizing the additional current drawn by the resistor (25mA for a 100Ω resistor and a 5V supply).

ESD PROTECTION

As stated in the Absolute Maximum Ratings, pin 6 (V_o3) on the LM4910 has a maximum ESD susceptibility rating of 10kV. For higher ESD voltages, the addition of a PCDN042 dual transil (from California Micro Devices), as shown in *Figure 4*, will provide additional protection.

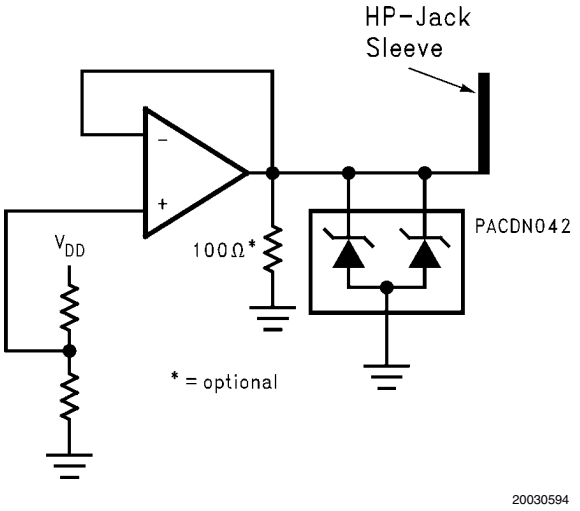


FIGURE 4. The PCDN042 provides additional ESD protection beyond the 10kV shown in the Absolute Maximum Ratings for the V_o3 output

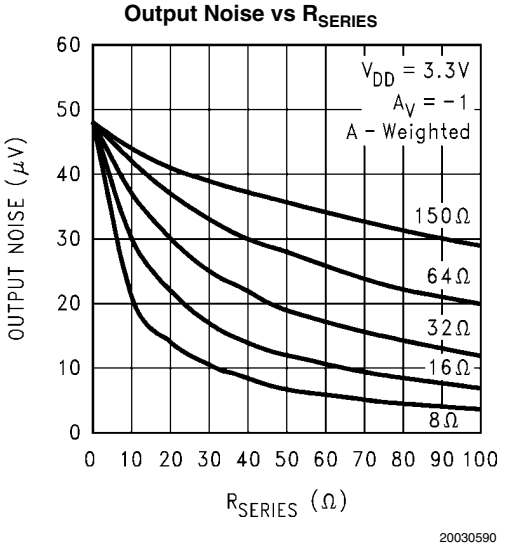


FIGURE 5.

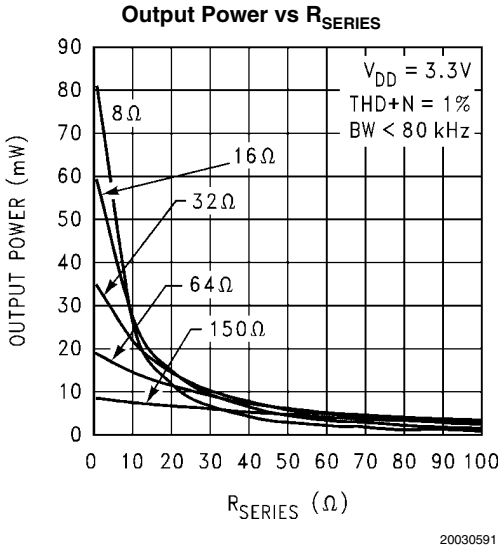


FIGURE 6.

HIGHER GAIN AUDIO AMPLIFIER

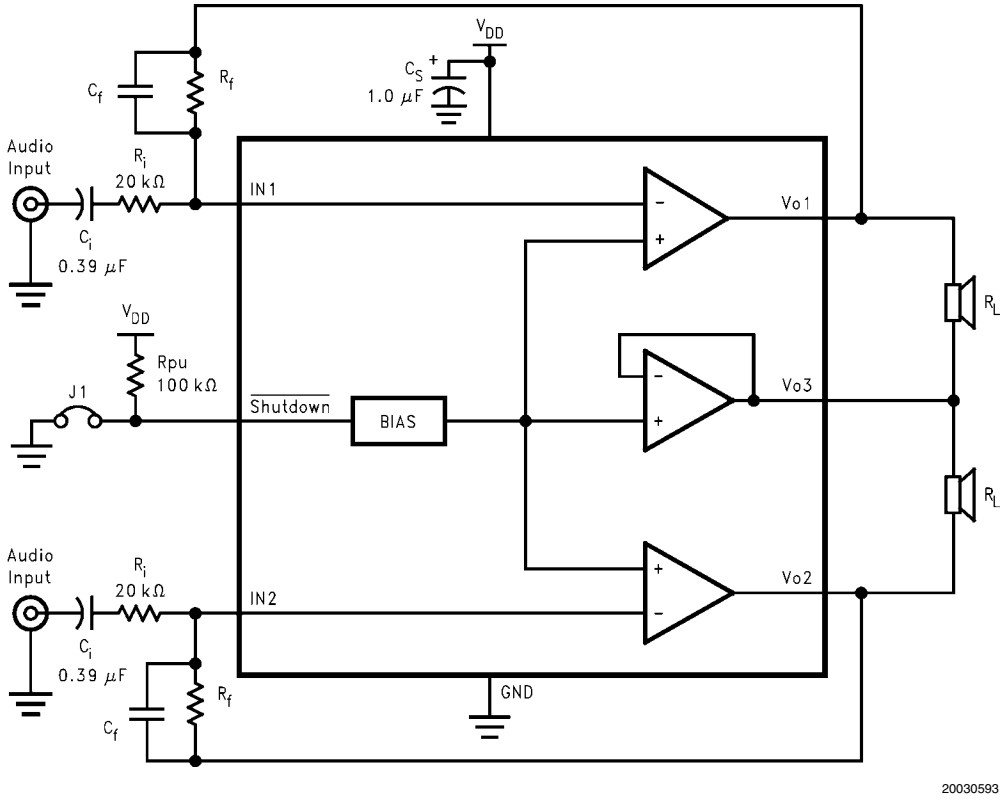


FIGURE 7.

The LM4910 is unity-gain stable and requires no external components besides gain-setting resistors, input coupling capacitors, and proper supply bypassing in the typical application. However, if a very large closed-loop differential gain is required, a feedback capacitor (C_f) may be needed as shown in *Figure 6* to bandwidth limit the amplifier. This feedback capacitor creates a low pass filter that eliminates possible high frequency oscillations. Care should be taken when calculating the -3dB frequency in that an incorrect combination of R_f and C_f will cause frequency response roll off before 20kHz. A typical combination of feedback resistor and capacitor that will not produce audio band high frequency roll off is Rf = 20kΩ and C_f = 25pF. These components result in a -3dB point of approximately 320kHz.

REFERENCE DESIGN BOARD and LAYOUT GUIDELINES
MSOP & SO BOARDS

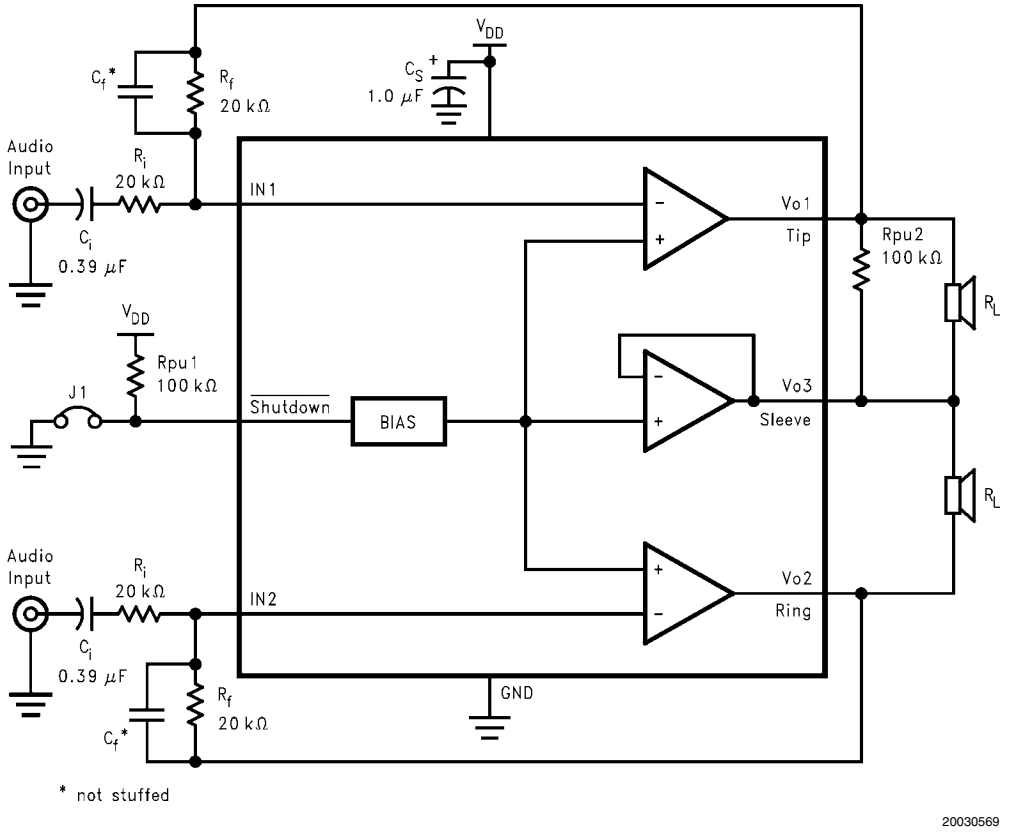
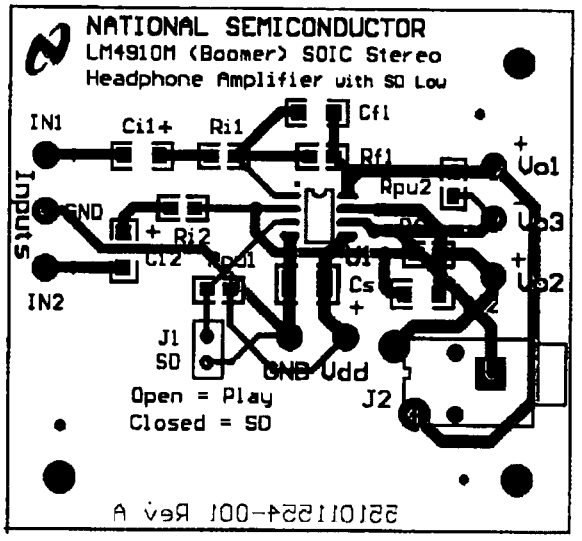


FIGURE 8.

(Note: $R_{PU}2$ is not required. It is used for test measurement purposes only.)

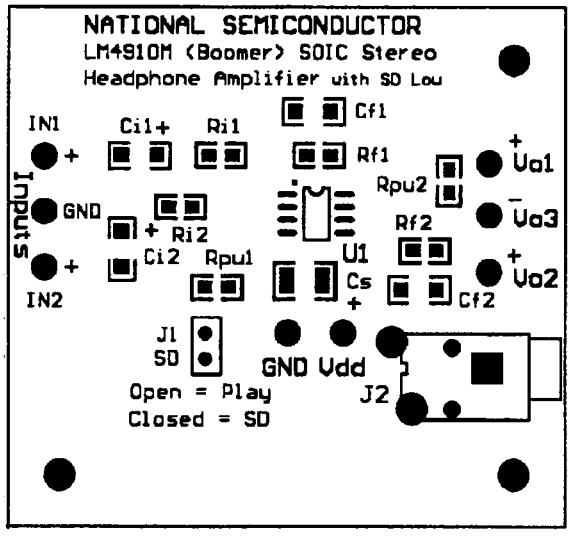
LM4910 SO DEMO BOARD ARTWORK

Composite View



20030570

Silk Screen



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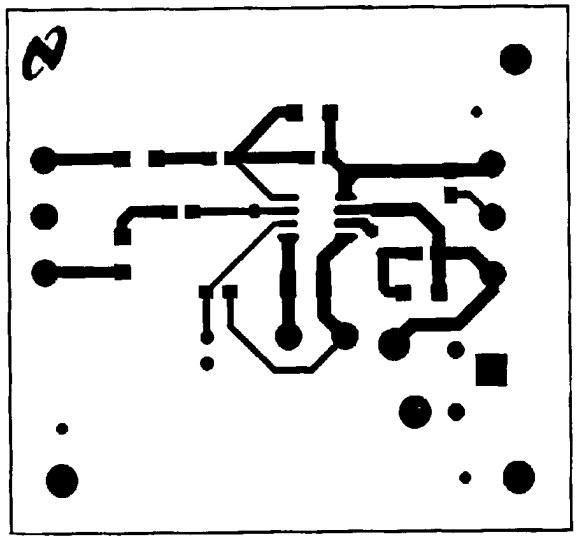
Top Layer



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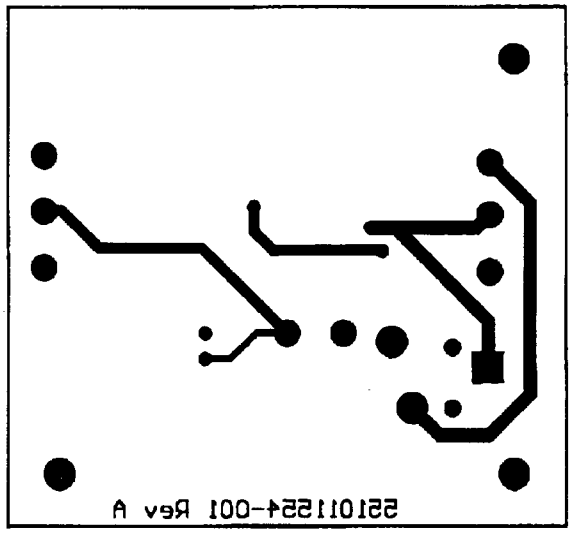
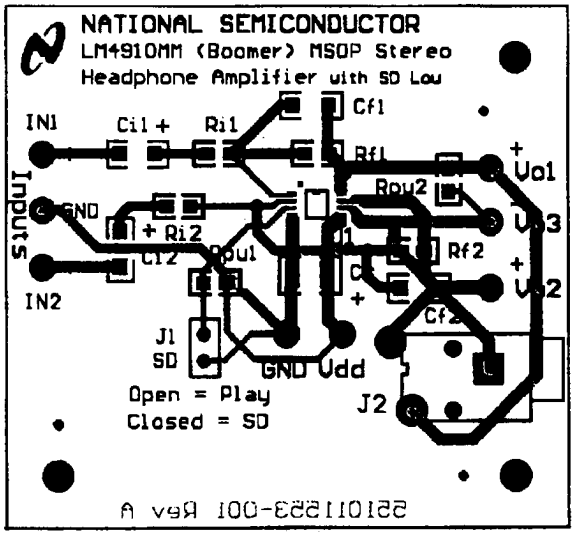


20030573

LM4910 MSOP DEMO BOARD ARTWORK

Composite View



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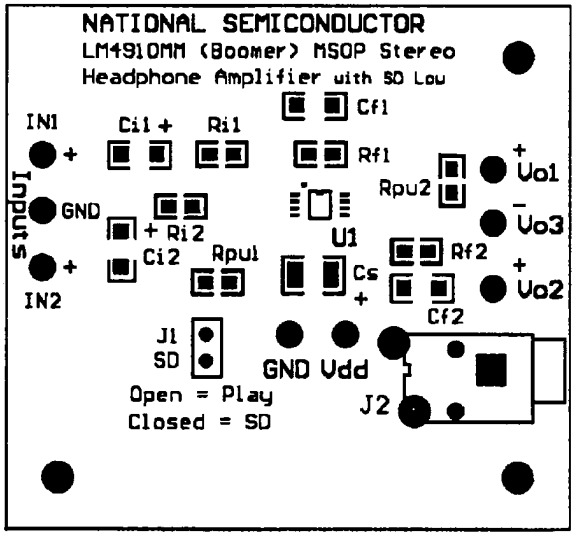

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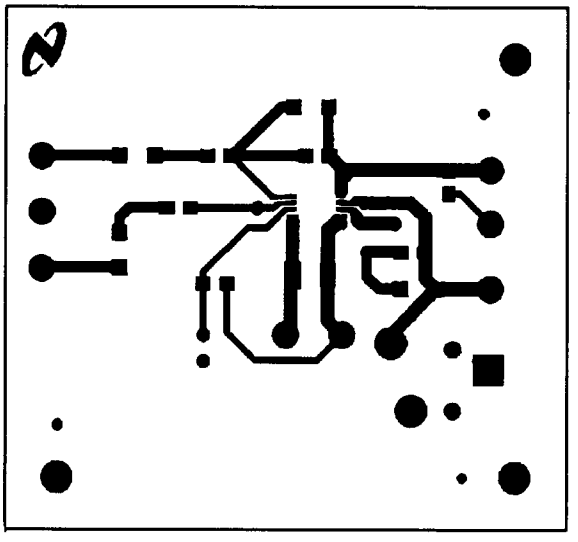

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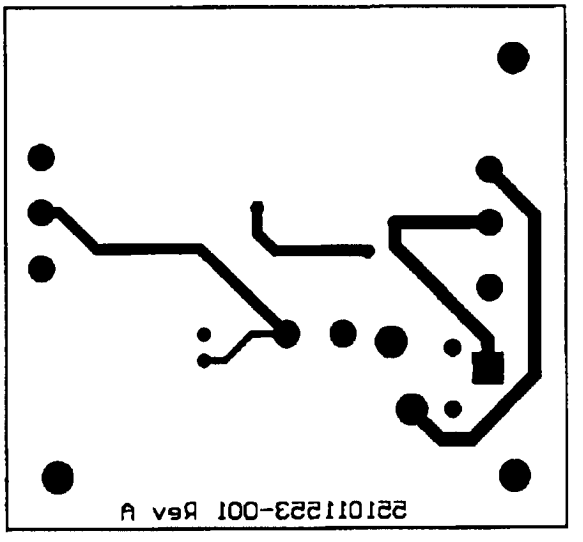
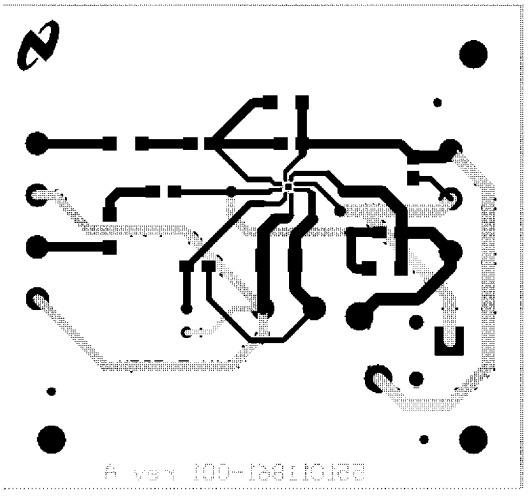


20030577

LM4910 LLP DEMO BOARD ARTWORK

Composite View



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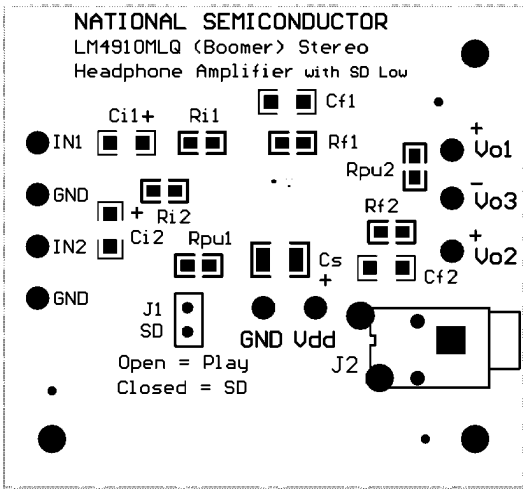

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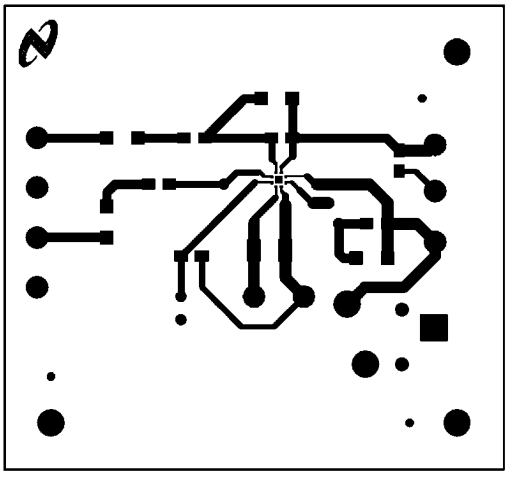

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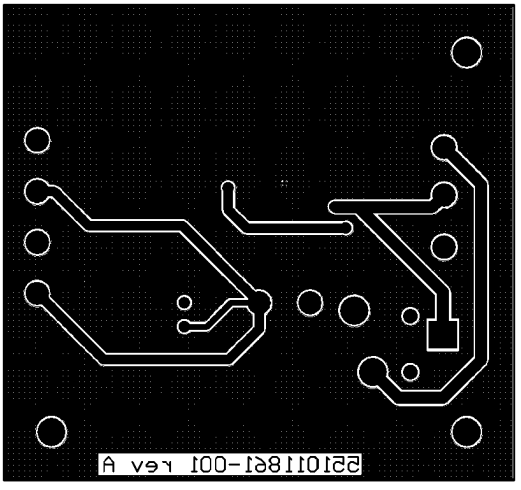


20030596

LM4910 Reference Design Boards
Bill of Materials

Part Description	Qty	Ref Designator
LM4910 Mono Reference Design Board	1	
LM4910 Audio AMP	1	U1
Tantalum Cap 1µF 16V 10	1	Cs
Ceramic Cap 0.39µF 50V Z50 20	2	Ci
Resistor 20kΩ 1/10W 5	4	Ri, Rf
Resistor 100kΩ 1/10W 5	1	Rpu
Jumper Header Vertical Mount 2X1, 0.100	1	J1

PCB LAYOUT GUIDELINES

This section provides practical guidelines for mixed signal PCB layout that involves various digital/analog power and ground traces. Designers should note that these are only "rule-of-thumb" recommendations and the actual results will depend heavily on the final layout.

Minimization of THD

PCB trace impedance on the power, ground, and all output traces should be minimized to achieve optimal THD performance. Therefore, use PCB traces that are as wide as possible for these connections. As the gain of the amplifier is increased, the trace impedance will have an ever increasing adverse affect on THD performance. At unity-gain (0dB) the parasitic trace impedance effect on THD performance is reduced but still a negative factor in the THD performance of the LM4910 in a given application.

GENERAL MIXED SIGNAL LAYOUT RECOMMENDATION

Power and Ground Circuits

For two layer mixed signal design, it is important to isolate the digital power and ground trace paths from the analog power and ground trace paths. Star trace routing techniques (bringing individual traces back to a central point rather than daisy chaining traces together in a serial manner) can greatly enhance low level signal performance. Star trace routing refers to using individual traces to feed power and ground to each circuit or even device. This technique will require a greater amount of design time but will not increase the final price of the board. The only extra parts required may be some jumpers.

Single-Point Power / Ground Connections

The analog power traces should be connected to the digital traces through a single point (link). A "PI-filter" can be helpful in minimizing high frequency noise coupling between the analog and digital sections. Further, place digital and analog power traces over the corresponding digital and analog ground traces to minimize noise coupling.

Placement of Digital and Analog Components

All digital components and high-speed digital signal traces should be located as far away as possible from analog components and circuit traces.

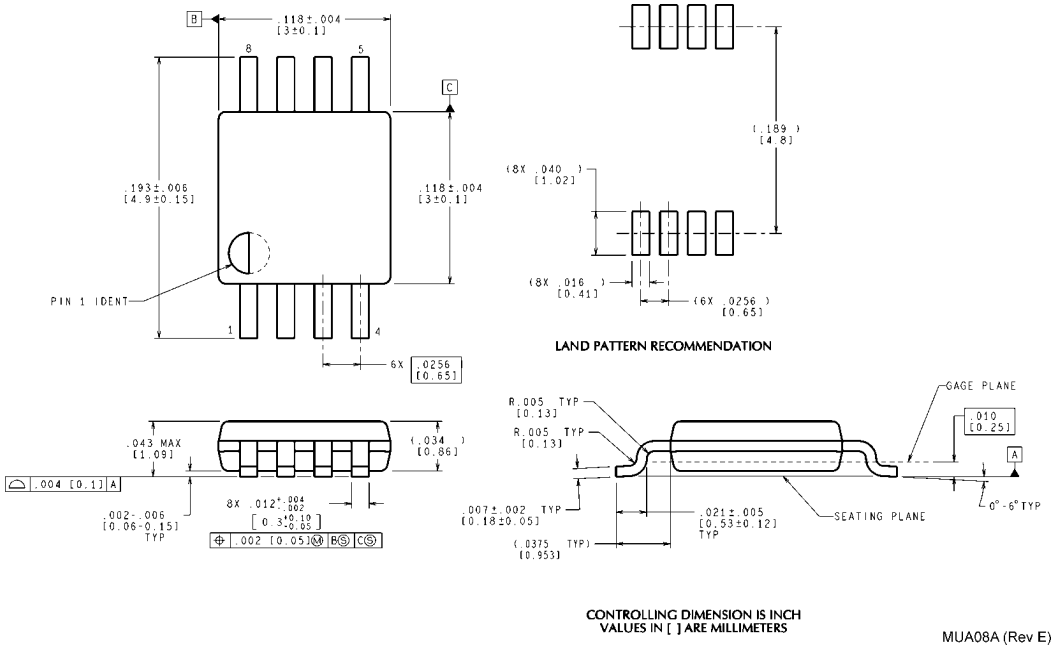
Avoiding Typical Design / Layout Problems

Avoid ground loops or running digital and analog traces parallel to each other (side-by-side) on the same PCB layer. When traces must cross over each other do it at 90 degrees. Running digital and analog traces at 90 degrees to each other from the top to the bottom side as much as possible will minimize capacitive noise coupling and cross talk.

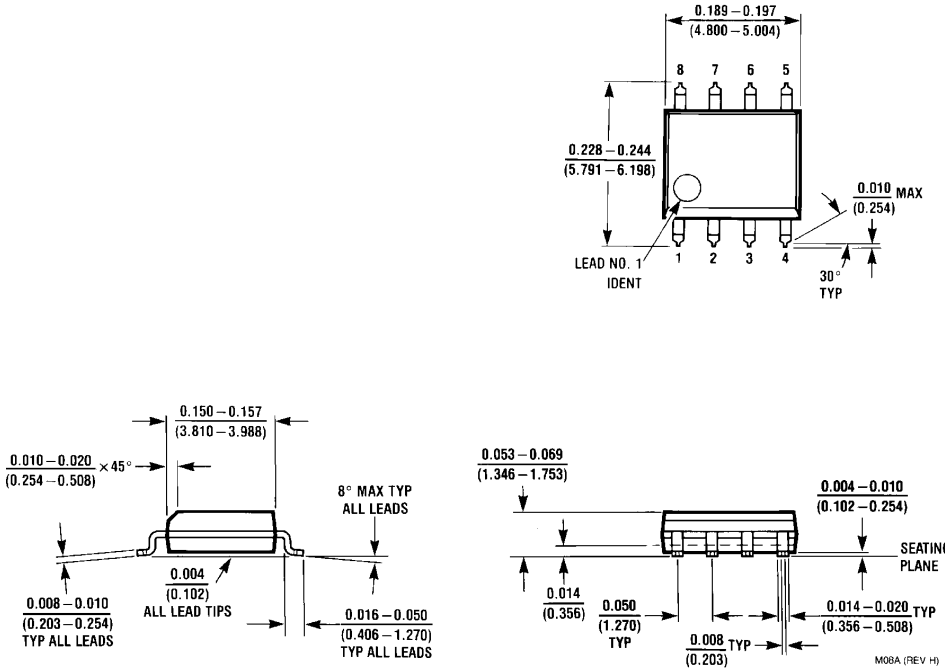
Revision History

Rev	Date	Description
1.0	7/12/05	Released to the WEB.
1.1	01/16/07	Deleted the phrase “patent pending” on page 1.

Physical Dimensions inches (millimeters) unless otherwise noted



MSOP
Order Number LM4910MM
NS Package Number MUA08A



SO
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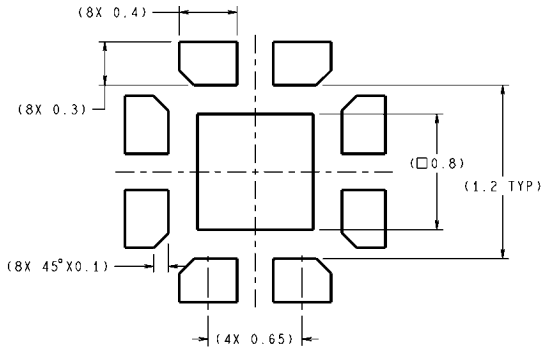
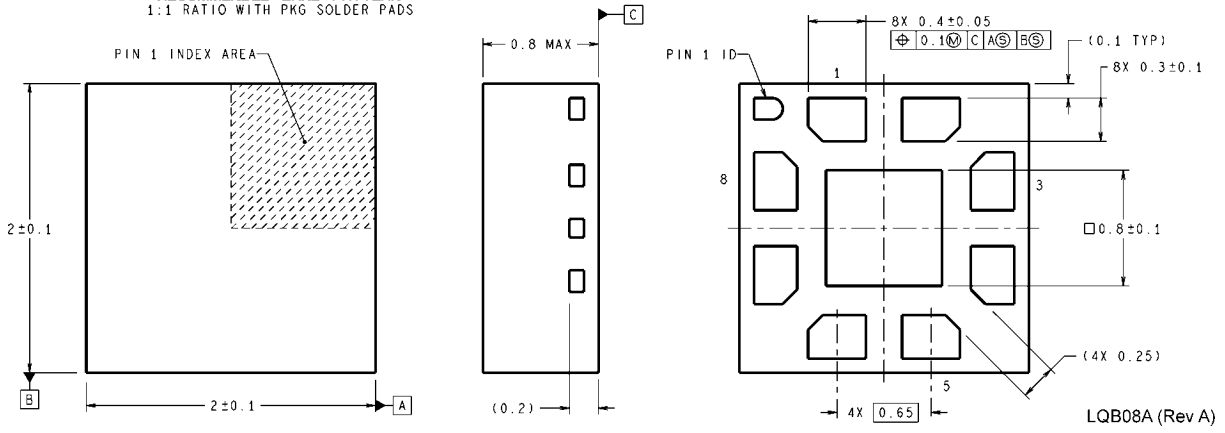
NS Package Number M08A



RECOMMENDED LAND PATTERN
1:1 RATIO WITH PKG SOLDER PADS

DIMENSIONS ARE IN MILLIMETERS



LQ
Order Number LM4910LQ
NS Package Number LQB08A

Notes

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